

DESCRIPTION

PLL FREQUENCY SYNTHESIZER

5 TECHNICAL FIELD

[0001] The present invention relates to a PLL frequency synthesizer for use in a semiconductor integrated circuit in the field of wireless communications and for generating a local signal required for transmission/reception of radio wave. More particularly, the present invention relates to an improvement in characteristics of the PLL frequency
10 synthesizer.

BACKGROUND ART

[0002] A structure of a conventional PLL frequency synthesizer is illustrated in FIG. 11.

15 [0003] The conventional PLL frequency synthesizer of FIG. 11 comprises a voltage control oscillator **VCO**, a programmable frequency divider **DIV**, a phase comparator **PFD**, a charge pump circuit **CP**, and a loop filter **LF**.

[0004] The voltage control oscillator **VCO** changes an oscillation frequency, depending on a potential of an oscillation frequency control signal V_T (described below).
20 The frequency divider **DIV** divides the oscillation frequency from the voltage control oscillator **VCO** with a frequency division ratio corresponding to an externally input channel selection signal. The phase comparator **PFD** detects a difference in phase between an output signal f_{DIV} from the frequency divider **DIV** and an externally input reference signal f_{REF} , and outputs a phase difference signal. The charge pump circuit **CP**
25 causes a current to flow into or out of an output point, depending on the phase difference signal from the phase comparator **PFD**. The loop filter **LF** filters out a high frequency component of an output current from the charge pump circuit **CP**, and converts the output

current into a direct current voltage value. An output of the loop filter **LF** is fed as the oscillation frequency control signal V_T back to the voltage control oscillator **VCO**.

[0005] An output frequency f_{out} of the thus-constructed conventional PLL frequency synthesizer is represented by a frequency represented by expression 1 below using a frequency f_{ref} of the reference signal and a division ratio N of the program frequency divider **DIV**.

$$[0006] \quad f_{out} = N \cdot f_{ref} \quad \dots\dots (1)$$

[0007] In actual radio transmitter-receivers, a predetermined output frequency f_{out} is obtained by changing the frequency f_{ref} of the reference signal or the frequency division ratio N , or both of them, and a signal of the output frequency f_{out} is used as a local signal for transmission/reception of a radio signal.

[0008] An open loop gain $GH(s)$ of the PLL frequency synthesizer is represented by expression 2 below.

$$[0009] \quad GH(s) = K_p \cdot Z_{lf}(s) \cdot \frac{K_{vco}}{s} \cdot \frac{1}{N} \quad \dots\dots (2)$$

[0010] In expression 2, K_{vco} is a sensitivity of the voltage control oscillator **VCO**, N is a frequency division number, $Z_{lf}(s)$ is a transfer function of a loop filter, K_p is a conversion gain of the phase comparator **PFD** and the charge pump circuit **CP**. The conversion gain K_p is represented by expression 3 below, where a charge pump current is indicated by I_{CP} .

$$K_p = \frac{I_{CP}}{2\pi} \quad \dots\dots (3)$$

[0011] [0012] The sensitivity K_{vco} of the voltage control oscillator **VCO** is represented by a proportion of a change in oscillation frequency with respect to a change in the input oscillation frequency control signal V_T . In an LC-type voltage control oscillator **LC-VCO** which is generally used as a PLL frequency synthesizer of a wireless

communications apparatus, the oscillation frequency control signal V_T is output to a variable capacitor, and the capacitance value of the variable capacitor varies depending on a voltage of the oscillation frequency control signal V_T , thereby changing an oscillation frequency of the voltage control oscillator **VCO**.

5 [0013] Here, the variable capacitance characteristics of a MOS-type variable capacitor which is frequently used as a variable capacitor or a p-n junction-type variable capacitor are generally nonlinear with respect to an input (i.e., the oscillation frequency control signal V_T). As a result, the oscillation frequency characteristics of the voltage control oscillator **VCO** are also nonlinear with respect to the input oscillation frequency control
10 signal V_T . A general voltage control oscillator **VCO** which employs a j-n junction capacitor as a variable capacitor has characteristics of an oscillation frequency f_{VCO} as illustrated in FIG. 12(a), and characteristics of the sensitivity K_{VCO} as illustrated in FIG. 12(b). Here, the charge pump current I_{CP} is a constant current as illustrated in FIG. 12(c). Therefore, the open loop gain $GH(s)$ of the PLL frequency synthesizer having such a
15 voltage control oscillator **VCO** is nonlinear as illustrated in FIG. 12(d), so that the loop gain characteristics of the whole PLL frequency synthesizer varies depending on the potential of the oscillation frequency control signal V_T . The variation of the loop gain characteristics due to the potential of the oscillation frequency control signal V_T is responsible for variation of a lock-up time, variation of phase noise characteristics, and the
20 like, i.e., degradation of characteristics.

[0014] In order to solve the above-described problem, a conventional technique is proposed in Patent Document 1. In this technique, the oscillation frequency control signal V_T is A/D converted, and a transient response in a convergence process of the PLL frequency synthesizer is detected by high-speed sampling using a DSP (Digital Signal
25 Processor) to obtain the sensitivity K_{VCO} of the voltage control oscillator **VCO**, and based on the result, the conversion gain K_p of the phase comparator **PFD** and the charge pump circuit **CP** is changed, thereby causing the transfer characteristics of the PLL frequency

synthesizer to be constant.

Patent Document 1: Japanese Patent Unexamined Publication No. H10-154934

DISCLOSURE OF THE INVENTION

5 PROBLEMS TO BE SOLVED BY THE INVENTION

[0015] However, in the conventional technique, an A/D converter, a DSP, and a D/A converter are required, so that the cost and the circuit area are significantly increased, and the circuit area of the whole PLL frequency synthesizer is inevitably increased. Therefore, the cost and size of a product into which the PLL frequency synthesizer is incorporated are
10 increased. In addition, noise which is generated in these circuits leads to a deterioration in characteristics of the PLL frequency synthesizer.

[0016] The present invention is provided to solve the above-described conventional problem. An object of the present invention is to minimize a variation in loop characteristics of a PLL frequency synthesizer without leading to a deterioration in
15 characteristics of the PLL frequency synthesizer while suppressing increases in the area and cost.

SOLUTION TO THE PROBLEMS

[0017] To achieve the above-described object, the present invention employs a simple
20 structure which changes a conversion gain of a phase comparator and a charge pump circuit without employing an A/D converter, a DSP, or a D/A converter which are used in conventional techniques.

[0018] Specifically, a PLL frequency synthesizer according to the present invention comprises a voltage control oscillator of changing an oscillation frequency, depending on a
25 potential of an oscillation frequency control signal, a frequency divider of dividing the oscillation frequency from the voltage control oscillator with a predetermined frequency division ratio, a phase comparator of receiving an output signal from the frequency divider

and an external reference signal, detecting a difference in phase between the output signal and the reference signal, and outputting a phase difference signal, a charge pump circuit of causing a constant current to flow in or out, depending on the phase difference signal from the phase comparator, a loop filter of filtering out a high frequency component of an output
5 of the charge pump circuit, converting the current flowing into or out of the charge pump circuit into a voltage, and outputting the voltage as the oscillation frequency control signal, and a linearization circuit of controlling a conversion gain of the phase comparator and the charge pump circuit so as to compensate for nonlinearity of a loop gain of the PLL frequency synthesizer with respect to the oscillation frequency control signal.

10 [0019] In the PLL frequency synthesizer of the present invention, the linearization circuit receives the oscillation frequency control signal from the loop filter, and continuously controls the conversion gain of the phase comparator and the charge pump circuit, depending on the potential of the oscillation frequency control signal.

[0020] In the PLL frequency synthesizer of the present invention, the linearization
15 circuit has a transistor, a current flowing through the transistor varying depending on the potential of the oscillation frequency control signal from the loop filter, and the linearization circuit continuously controls the conversion gain of the phase comparator and the charge pump circuit, depending on a value of the current flowing through the transistor.

[0021] In the PLL frequency synthesizer of the present invention, the transistor of the
20 linearization circuit is composed of a plurality of transistors, and the conversion gain of the phase comparator and the charge pump circuit is continuously controlled, depending on a sum of currents flowing through the plurality of transistors.

[0022] In the PLL frequency synthesizer of the present invention, the plurality of transistors of the linearization circuit have different threshold voltages from each other.

25 [0023] In the PLL frequency synthesizer of the present invention, the linearization circuit has a bias voltage generating circuit of generating a bias voltage, the bias voltage of the bias voltage generating circuit is input to a source of the transistor of the linearization

circuit, and the oscillation frequency control signal from the loop filter is input to a gate of the transistor, and the conversion gain of the phase comparator and the charge pump circuit is continuously controlled, depending on a value of the current flowing through the transistor.

5 [0024] In the PLL frequency synthesizer of the present invention, the transistor of the linearization circuit is composed of a plurality of transistors, and the conversion gain of the phase comparator and the charge pump circuit is continuously controlled, depending on a sum of currents flowing through the plurality of transistors.

[0025] In the PLL frequency synthesizer of the present invention, the bias voltage
10 generating circuit generates a plurality of different bias voltages, and the different bias voltages from the bias voltage generating circuit are input to respective sources of the plurality of transistors of the linearization circuit.

[0026] In the PLL frequency synthesizer of the present invention, the bias voltage
15 generating circuit changes the plurality of generated bias voltages based on an externally input bias voltage setting signal.

[0027] In the PLL frequency synthesizer of the present invention, the plurality of transistors of the linearization circuit are composed of a P-type or N-type MOS transistor or P-type and N-type MOS transistors.

[0028] In the PLL frequency synthesizer of the present invention, the linearization
20 circuit comprises a voltage-current conversion circuit of converting a voltage of the oscillation frequency control signal from the loop filter into a current, and a charge pump current control circuit of receiving the current from the voltage-current conversion circuit, generating a charge pump current control signal corresponding to a value of the received current, and outputting the charge pump current control signal to the charge pump circuit.
25 The charge pump circuit regulates a flowing current based on the charge pump current control signal from the charge pump current control circuit.

[0029] Thus, according to the present invention, the linearization circuit continuously

controls the conversion gain of the phase comparator and the charge pump circuit, depending on, for example, the potential of the oscillation frequency control signal from the loop filter. Therefore, the loop gain characteristics of the PLL frequency synthesizer can be regulated to be constant without depending on the potential of the oscillation frequency control signal, using a relatively simple structure employing the linearization circuit, and without using an A/D converter, a DSP, or a D/A converter which are used in conventional techniques.

[0030] Particularly, in the present invention, the linearization circuit controls the conversion gain of the phase comparator and the charge pump circuit by utilizing a change in the current drive ability of a transistor with respect to an input voltage. Therefore, with the simpler structure, the loop gain characteristics of the PLL frequency synthesizer can be regulated to be constant.

EFFECT OF THE INVENTION

[0031] As described above, according to the present invention, the linearization circuit is used so as to continuously control the conversion gain of the phase comparator and the charge pump circuit. Therefore, with a structure simpler than conventional structures, the loop gain characteristics of the PLL frequency synthesizer can be regulated to be constant. Therefore, a variation in lock-up time, a variation in phase noise characteristics, and the like can be suppressed over a broad band. Therefore, an inexpensive and high-performance broad-band PLL frequency synthesizer required in the field of broad-band wireless communications can be provided.

[0032] Particularly, according to the present invention, the loop gain characteristics of the PLL frequency synthesizer can be regulated to be constant using a simpler structure.

BRIEF DESCRIPTION OF THE DRAWINGS

[0033] [FIG. 1] FIG. 1 illustrates a structure of a PLL frequency synthesizer according

to a first embodiment of the present invention.

[FIG. 2] FIG. 2 is a diagram illustrating a structure of a linearization circuit included in the PLL frequency synthesizer.

[FIG. 3] FIG. 3 is a diagram illustrating a specific structure of the linearization circuit.

[FIG. 4] FIG. 4(a) is a diagram illustrating oscillation frequency characteristics of a voltage control oscillator included in the PLL frequency synthesizer of the first embodiment of the present invention. FIG. 4(b) is a diagram illustrating sensitivity characteristics thereof. FIG. 4(c) is a diagram illustrating charge pump current characteristics thereof. FIG. 4(d) is a diagram illustrating loop gain characteristics of the PLL frequency synthesizer.

[FIG. 5] FIG. 5 is a diagram illustrating a specific structure of a linearization circuit included in a PLL frequency synthesizer according to a second embodiment of the present invention.

[FIG. 6] FIG. 6 is a diagram illustrating current characteristics of a charge pump included in the PLL frequency synthesizer.

[FIG. 7] FIG. 7 is a diagram illustrating a specific structure of a linearization circuit included in a PLL frequency synthesizer according to a third embodiment of the present invention.

[FIG. 8] FIG. 8 is a diagram illustrating a specific structure of a linearization circuit included in a PLL frequency synthesizer according to a fourth embodiment of the present invention.

[FIG. 9] FIG. 9 is a diagram illustrating a specific structure of a linearization circuit included in a PLL frequency synthesizer according to a fifth embodiment of the present invention.

[FIG. 10] FIG. 10(a) is a diagram illustrating oscillation frequency characteristics of a voltage control oscillator included in the PLL frequency synthesizer of the fifth

embodiment of the present invention. FIG. 10(b) is a diagram illustrating sensitivity characteristics thereof. FIG. 10(c) is a diagram illustrating charge pump current characteristics thereof. FIG. 10(d) is a diagram illustrating loop gain characteristics of the PLL frequency synthesizer.

5 [FIG. 11] FIG. 11 is a diagram illustrating a structure of a conventional PLL frequency synthesizer.

[FIG. 12] FIG. 12(a) is a diagram illustrating oscillation frequency characteristics of a voltage control oscillator included in the conventional PLL frequency synthesizer. FIG. 12(b) is a diagram illustrating sensitivity characteristics thereof. FIG. 12(c) is a
10 diagram illustrating charge pump current characteristics thereof. FIG. 12(d) is a diagram illustrating loop gain characteristics of the conventional PLL frequency synthesizer.

DESCRIPTION OF THE REFERENCE CHARACTERS

[0034]	VCO	voltage control oscillator
15	VIV	programmable frequency divider
	PED	phase comparator
	CP	charge pump circuit
	LF	loop filter
	6, 6', 6'', 6''', 6''''	linearization circuit
20	7, 7', 7'', 7''', 7''''	V-I conversion circuit (voltage-current conversion circuit)
	8, 8'	CP bias control circuit
		(charge pump current control circuit)
	MN1, MN1A, MN1B	N-type transistor (transistor)
	V_T	oscillation frequency control signal
25	CP_{CONT}	charge pump current control signal

BEST MODE FOR CARRYING OUT THE INVENTION

[0035] Hereinafter, PLL frequency synthesizers according to embodiments of the present invention will be described with reference to the accompanying drawings.

[0036] (First embodiment)

FIG. 1 illustrates a structure of a PLL frequency synthesizer according to a first embodiment of the present invention.

[0037] In FIG. 1, the PLL frequency synthesizer comprises a voltage control oscillator **VCO**, a programmable frequency divider **DIV**, a phase comparator **PFD**, a charge pump circuit **CP**, and a loop filter **LF**.

[0038] The voltage control oscillator **VCO** changes an oscillation frequency, depending on a voltage of an oscillation frequency control signal V_T . The frequency divider **DIV** divides an oscillation frequency f_{OUT} from the voltage control oscillator **VCO** with a frequency division ratio corresponding to an externally input channel selection signal. The phase comparator **PFD** detects a difference in phase between an output signal f_{DIV} from the frequency divider **DIV** and an externally input reference signal f_{REF} , and outputs a phase difference signal. The charge pump circuit **CP** causes a current to flow into or out of an output point, depending on the phase difference signal from the phase comparator **PFD**. The loop filter **LF** filters out high frequency components of an output current from the charge pump circuit **CP**, and converts the output current into a direct current voltage value. An output of the loop filter **LF** is fed as the oscillation frequency control signal V_T back to the voltage control oscillator **VCO**.

[0039] In the first embodiment of the present invention, a linearization circuit **6** is further provided which continuously controls a conversion gain K_p of the phase comparator **PFD** and the charge pump circuit **CP** so as to compensate for nonlinearity of a sensitivity (specifically, a proportion of a change in the output oscillation frequency f_{OUT}) of the voltage control oscillator **VCO** with respect to the oscillation frequency control signal V_T . Hereinafter, the linearization circuit **6** will be described.

[0040] An internal structure of the linearization circuit **6** is illustrated in FIG. 2. The

linearization circuit 6 of FIG. 2 comprises a V-I conversion circuit (voltage-current conversion circuit) 7 and a charge pump bias current control circuit (hereinafter abbreviated as a CP bias control circuit) 8. The V-I conversion circuit 7 receives the oscillation frequency control signal V_T from the loop filter LF, and converts a potential level of the oscillation frequency control signal V_T into a current value $V-I_{OUT}$ corresponding to the potential level. The CP bias control circuit (charge pump current control circuit) 8 outputs a charge pump current control signal CP_{CONT} which controls a bias current value of a charge pump current I_{CP} of the charge pump circuit CP, depending on the current value $V-I_{OUT}$ obtained by the V-I conversion circuit 7.

[0041] Specific internal structures of the V-I conversion circuit 7 and the CP bias control circuit 8 in the linearization circuit 6 of FIG. 2 are illustrated in FIG. 3. Referring to FIG. 3, in the V-I conversion circuit 7, a series circuit of a P-type transistor MP1 and an N-type transistor MN1 is provided between a power source and a ground. The oscillation frequency control signal V_T is input from the loop filter LF to a gate of the N-type transistor MN1, and a value of a current I_1 which flows through the N-type transistor MN1 varies depending on a potential of the oscillation frequency control signal V_T . Specifically, as the potential of the oscillation frequency control signal V_T is increased, the current drive capability of the N-type transistor MN1 increases, resulting in an increase in the current value I_1 .

[0042] In the CP bias control circuit 8 of FIG. 3, a P-type transistor MP2 is provided, and the P-type transistor MP2 and the P-type transistor MP1 of the V-I conversion circuit 7 constitute a current mirror circuit, which mirrors the current value I_1 flowing through the N-type transistor MN1 of the V-I conversion circuit 7, so that the current value I_1 is input to the CP bias control circuit 8. The CP bias control circuit 8 also comprises a current mirror circuit composed of two P-type transistors MP3 and MP4 and a reference current source 10, which generate a current I_0 . The current I_0 and the input current value I_1 (a total current value I_0+I_1) is caused to flow through an N-type transistor MN2, and the

current value $I_0 + I_1$ is supplied as the charge pump current control signal CP_{CONT} from a node (a gate electrode of the N-type transistor MN2) to the charge pump circuit CP of FIG. 1 so that the charge pump current I_{CP} of the charge pump circuit CP is controlled. For example, a current proportional to a value of the charge pump current control signal CP_{CONT} may be caused to flow from the charge pump circuit CP, though the drawings do not illustrate how to control the charge pump current I_{CP} using the charge pump current control signal CP_{CONT} .

[0043] FIG. 4 illustrates loop gain characteristics of each part of and the whole PLL frequency synthesizer of the first embodiment of the present invention. FIG. 4(a) illustrates characteristics of the oscillation frequency f_{VCO} of a general voltage control oscillator VCO which employs a p-n junction-type variable capacitor. FIG. 4(b) illustrates characteristics of the sensitivity K_{VCO} of the voltage control oscillator VCO. As can be seen from FIGS. 4(a) and 4(b), a proportion of a change in the oscillation frequency f_{VCO} , and the sensitivity K_{VCO} decreases with an increase in the potential of the oscillation frequency control signal V_T . FIG. 4(c) illustrates current characteristics of the charge pump circuit CP. A dashed line illustrated in FIG. 4(c) indicates the charge pump current I_{CP} of the conventional example of FIG. 1, which has a constant value. In the first embodiment of the present invention, as illustrated with a solid line, the charge pump current I_{CP} increases with an increase in the potential of the oscillation frequency control signal V_T , due to the linearization circuit 8. Therefore, as illustrated in FIG. 4(d), characteristics of the loop gain $GH(s)$ of the whole PLL frequency synthesizer are proportional to the characteristics of the sensitivity K_{VCO} of the voltage control oscillator VCO multiplied by the current I_{CP} of the charge pump circuit CP. Therefore, in the conventional example, as illustrated with a dashed line in FIG. 4(d), the characteristics of the loop gain $GH(s)$ of the whole PLL frequency synthesizer monotonically decreases with an increase in the potential of the oscillation frequency control signal V_T , and the variation with respect to the oscillation frequency control signal V_T is large. In the first

embodiment of the present invention, the variation can be reduced due to the linearization circuit 8 as illustrated with a solid line in FIG. 4(d).

[0044] As described above, in the PLL frequency synthesizer of the first embodiment of the present invention, the linearization circuit 8 of FIG. 3 which has a considerably simple structure is only added, thereby making it possible to obtain substantially constant characteristics of the loop gain $GH(s)$ of the whole PLL frequency synthesizer without depending on the potential level of the oscillation frequency control signal V_T . Therefore, the effect of reducing variations in lock time and phase noise characteristics of the PLL frequency synthesizer can be achieved over a broad band with a considerably small increase in circuit scale.

[0045] (Second embodiment)

Next, a second embodiment of the present invention will be described. The second embodiment of the present invention is provided with a variation of the linearization circuit 6 of the first embodiment.

[0046] Specifically, the linearization circuit 6' of FIG. 5 has a V-I conversion circuit 7' in which a series circuit of a P-type transistor MP1A and an N-type MN1A and a series circuit of a P-type transistor MP1B and an N-type MN1B are provided. The oscillation frequency control signal V_T is input from the loop filter LF to a gate of each of the two N-type transistors MN1A and MN1B. Therefore, as is similar to the V-I conversion circuit 7 of FIG. 3, currents I_{1A} and I_{1B} flowing through the respective N-type transistors MN1A and MN1B of the two series circuits vary depending on the potential of the oscillation frequency control signal V_T input to the respective gates. A CP bias control circuit 8' comprises two P-type transistors MP2A and MP2B for receiving a current. The two currents I_{1A} and I_{1B} flowing through the V-I conversion circuit 7' are input to the CP bias control circuit 8' due to a current mirror structure. The two input current I_{1A} and I_{1B} are added with a reference current I_0 as illustrated in FIG. 6, and the resultant sum current is input as a charge pump current control signal CP_{CONT} from a gate electrode of the N-type

transistor **MN2** to the charge pump circuit **CP** of FIG. 1.

[0047] Here, in the V-I conversion circuit 7', the two N-type transistors **MN1A** and **MN1B** have different threshold voltages, so that the flowing current amounts I_{1A} and I_{1B} are different from each other due to a difference in current drive ability even if the bias voltage value (oscillation frequency control signal V_T) is the same. Therefore, in the second embodiment of the present invention, it is possible to more finely control the charge pump current control signal **CP_{CONT}** from the CP bias control circuit 8' with respect to a change in the oscillation frequency control signal V_T . Therefore, the dependence of the charge pump current I_{CP} on the potential of the oscillation frequency control signal V_T can be made close to the sensitivity characteristics of the voltage control oscillator **VCO**, thereby making it possible to further reduce a variation in the PLL frequency synthesizer due to a change in the potential of the oscillation frequency control signal V_T .

[0048] Although, in the second embodiment of the present invention, the two N-type transistors **MN1A** and **MN1B** have different threshold voltages from each other so as to finely control the charge pump current control signal **CP_{CONT}**, three or more N-type transistors may be provided. In addition, a current flowing through each N-type transistor may be controlled using a parameter other than the threshold voltage so as to finely control the charge pump current control signal **CP_{CONT}**.

[0049] (Third embodiment)

Next, a third embodiment of the present invention will be described. The third embodiment of the present invention is provided with another variation of the linearization circuit 6 of the first embodiment.

[0050] Specifically, the linearization circuit 6'' of FIG. 7 has a V-I conversion circuit 7'' in which an N-type transistor **MN3** is provided between a source of an N-type transistor **MN1** to a gate of which an oscillation frequency control signal V_T is input, and a ground. An operational amplifier 12 is connected to a gate of the N-type transistor **MN3**. A source voltage of the N-type transistor **MN1** and a bias voltage generated in a bias

voltage generating circuit 11 are input to the operational amplifier 12. The operational amplifier 12 controls the N-type transistor MN3 so that a source voltage of the N-type transistor MN1 becomes equal to the bias voltage generated by the bias voltage generating circuit 11. Note that a CP bias control circuit 8 of FIG. 7 has the same structure as that of the CP bias control circuit 8 of FIG. 1.

[0051] Therefore, a current I1 flowing through the N-type transistor MN1 of the V-I conversion circuit 7'' is determined, depending on the bias voltage of the bias voltage generating circuit 11 and the potential of the oscillation frequency control signal V_T of the loop filter LF. Therefore, by setting the bias voltage of the bias voltage generating circuit 11 to be various values based on an externally input bias voltage setting signal, the charge pump current control signal CP_{CONT} from the CP bias control circuit 8 can be more finely controlled than in the first and second embodiments, thereby making it possible to further suppress a variation in the loop gain of the PLL frequency synthesizer due to the potential of the oscillation frequency control signal V_T .

[0052] (Fourth embodiment)

Further, a fourth embodiment of the present invention will be described. The fourth embodiment of the present invention is provided with a variation of the linearization circuit 6' of the second embodiment.

[0053] Specifically, the linearization circuit 6''' of FIG. 8 has an additional structure in which the V-I conversion circuit 7' of FIG. 5 is further provided with the bias voltage generating circuit 11 of FIG. 7. Specifically, in a V-I conversion circuit 7''', N-type transistors MN3A and MN3B are provided between sources of respective N-type transistors MN1A and MN1B to gates of which an oscillation frequency control signal V_T is input, and a ground. Operational amplifiers 12A and 12B are connected to gates of the respective N-type transistors MN3A and MN3B. A source voltage of the N-type transistor MN1A and a first bias voltage of the bias voltage generating circuit 11 are input to the operational amplifier 12, while a source voltage of the N-type transistor MN1B and

a second bias voltage of the bias voltage generating circuit **11** are input to the operational amplifier **12B**.

[0054] Therefore, in the fourth embodiment of the present invention, by setting the threshold voltages of the N-type transistors **MN1A** and **MN1B** to obtain an appropriate current drive ability and controlling the first and second bias voltage values of the bias voltage generating circuit **11**, a charge pump current I_{CP} which satisfactorily compensates for the nonlinearity of the sensitivity of the voltage control oscillator **VCO** with respect to the oscillation frequency control signal V_T , can be generated, thereby making it possible to considerably suppress a variation in the loop gain characteristics of the whole PLL frequency synthesizer.

[0055] Although, in the fourth embodiment of the present invention, the number of the N-type transistors **MN1A** and **MN1B** to the gates of which the oscillation frequency control signal V_T is input is two and the number of bias voltages generated by the bias voltage generating circuit **11** is two, the number of N-type transistors and the number of generated bias voltages may be each three or more.

[0056] (Fifth embodiment)

Next, a fifth embodiment of the present invention will be described. The fifth embodiment of the present invention is provided with a variation of the linearization circuit **6'''** of the second embodiment.

[0057] Specifically, the linearization circuit **6'''** of FIG. 9 has a V-I conversion circuit **7'''** composed of two N-type transistors **MN1A** and P-type transistor **MP1B** to gates of which an oscillation frequency control signal V_T is input. Further, the linearization circuit **6'''** is further provided with P-type and N-type transistors **MP4** and **MN4** for outputting a current I_{IB} flowing through a series circuit composed of the P-type transistor **MP1B** and the N-type transistor **MN1B** to the outside by means of a current mirror structure.

[0058] Therefore, in the fifth embodiment of the present invention, when the potential

of the oscillation frequency control signal V_T is increased to be larger than a bias voltage input to a source of the N-type transistor **MN1A** by a threshold voltage of the N-type transistor **MN1A** or more, a current flows through the N-type transistor **MN1A**. When the potential of the oscillation frequency control signal V_T is decreased to be smaller than a bias voltage input to a source of the P-type transistor **MP1B** by a threshold voltage of the P-type transistor **MP1B** or more, a current flows through the P-type transistor **MP1B**.

[0059] When a MOS-type variable capacitor is used as a variable capacitor, the oscillation frequency f_{VCO} of a general voltage control oscillator **VCO** has characteristics as illustrated in FIG. 10(a), and the sensitivity K_{VCO} thereof has characteristics as illustrated in FIG. 10(b). Here, the charge pump current I_{CP} from the charge pump circuit **CP** which is controlled using the charge pump current control signal CP_{CONT} from the CP bias control circuit 8' increases due to the current I_{IB} flowing through the P-type transistor **MP1B** when the potential of the oscillation frequency control signal V_T is low, as illustrated in FIG. 10(c). The charge pump current I_{CP} also increases due to the current I_{IA} flowing through the N-type transistor **MN1A** when the potential of the oscillation frequency control signal V_T is high. Therefore, the charge pump current I_{CP} compensates for the nonlinearity of the sensitivity characteristics of the voltage control oscillator **VCO**. As illustrated in FIG. 10(d), in a conventional example indicated with a solid line, characteristics of a loop gain $GH(s)$ of the PLL frequency synthesizer vary largely, depending on a variation in the potential of the oscillation frequency control signal V_T . On the other hand, in the fifth embodiment of the present invention indicated with a solid line, the characteristics of the loop gain $GH(s)$ of the PLL frequency synthesizer can have substantially a constant value with respect to the potential of the oscillation frequency control signal V_T over a broad range, so that the effect of reducing a variation in the loop gain characteristics of the PLL frequency synthesizer is significant.

[0060] Note that an output bias voltage can be variably controlled by the bias voltage generating circuit 11 of FIGS. 7, 8, and 9 using an externally input bias voltage setting

signal, and therefore, it is possible to set an optimal bias voltage, taking into consideration, for example, a variation in characteristics of the sensitivity K_{VCO} of the voltage control oscillator VCO and a variation in current drive ability of a transistor constituting the linearization circuits 6'', 6''', and 6'''' when the PLL frequency synthesizer is
5 manufactured.

INDUSTRIAL APPLICABILITY

[0061] As described above, according to the present invention, a linearization circuit which controls a conversion gain of a phase comparator and a charge pump circuit,
10 depending on an oscillation frequency control signal from a loop filter, is used to compensate for the nonlinearity of the sensitivity characteristics of a voltage control oscillator with respect to the potential of an oscillation frequency control signal so that loop gain characteristics of a PLL frequency synthesizer are constant without depending on the potential of the oscillation frequency control signal. Therefore, the present invention
15 is useful in applications, such as a PLL frequency synthesizer of a relatively broad band in the field of communications, and the like.